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Saunders

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[54] **APPARATUS AND METHOD FOR ADAPTIVE BEAMFORMING IN AN ANTENNA ARRAY**

[75] Inventor: **Simon Saunders**, Guildford, United Kingdom

[73] Assignee: **Motorola, Inc.**, Schaumburg, Ill.

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[51] **Int. Cl.**^{7} **H04B 7/02**; H04L 1/02

[52] **U.S. Cl.** **375/267**; 455/226.2

[58] **Field of Search** 375/267, 260, 375/259; 455/562, 226.1, 226.2, 226.3

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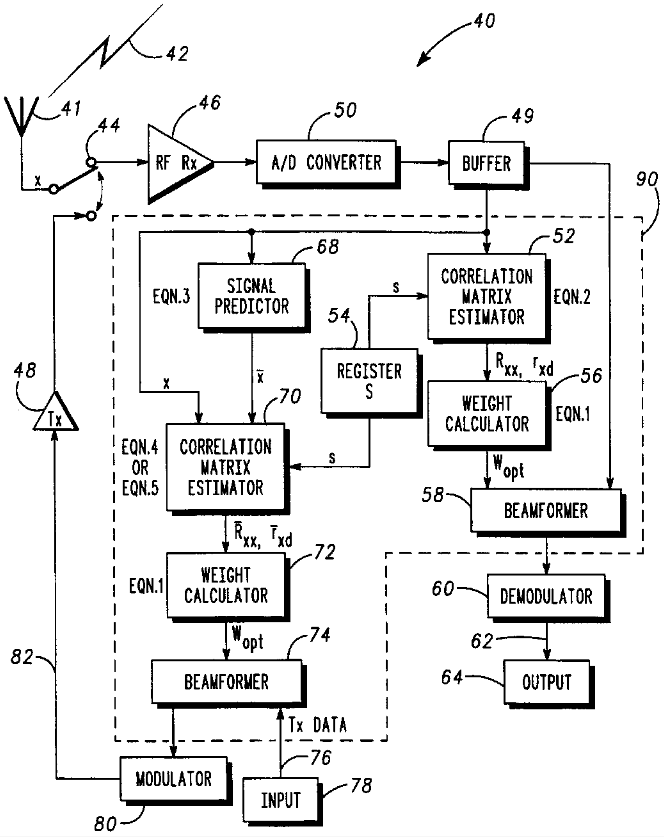
Primary Examiner—Don N. Vo
Assistant Examiner—Phuong Phu
Attorney, Agent, or Firm—Heather L. Creps

[57] **ABSTRACT**

An apparatus and a method for receiving and transmitting information from an array of adaptive antenna elements, wherein a predictive filter supplies an estimate of received signal samples likely to be received in a burst immediately preceding a transmission. Combination of this estimate with received signal samples obtained from actual (historically received) signals, received over a predetermined number of frames, yield estimates of optimum beamforming coefficients for application to data for transmission from an adaptive array of antenna elements. As such, available processing time for obtaining the beamforming coefficients is increased.

10 Claims, 2 Drawing Sheets



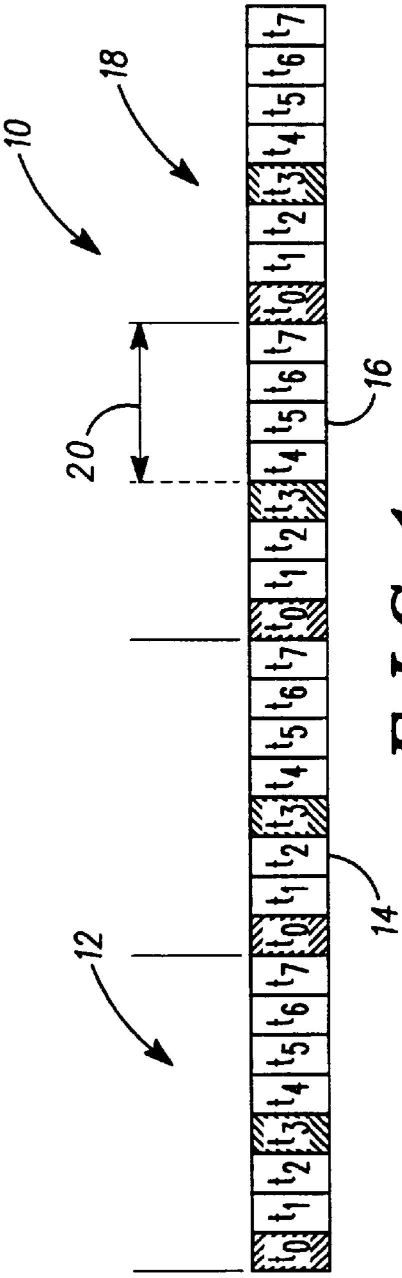


FIG. 1
PRIOR ART

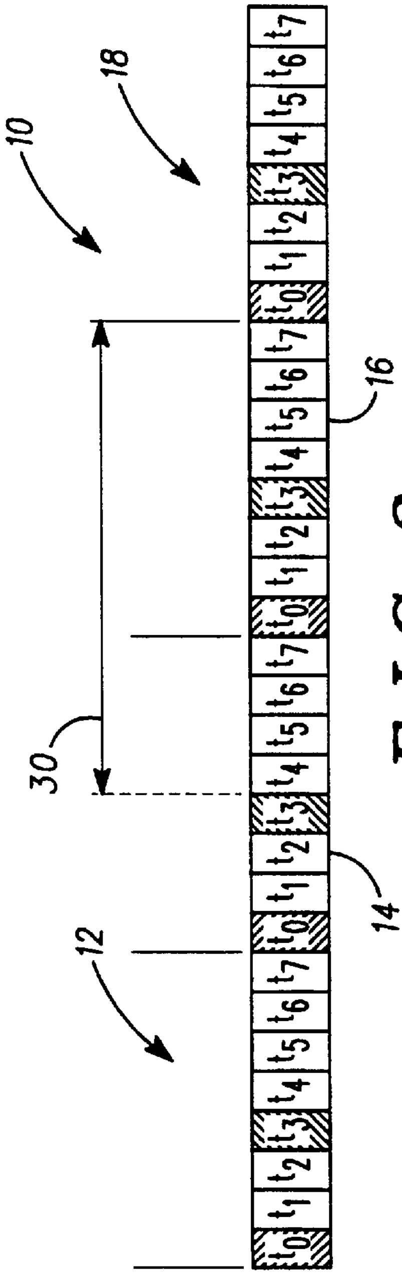


FIG. 2

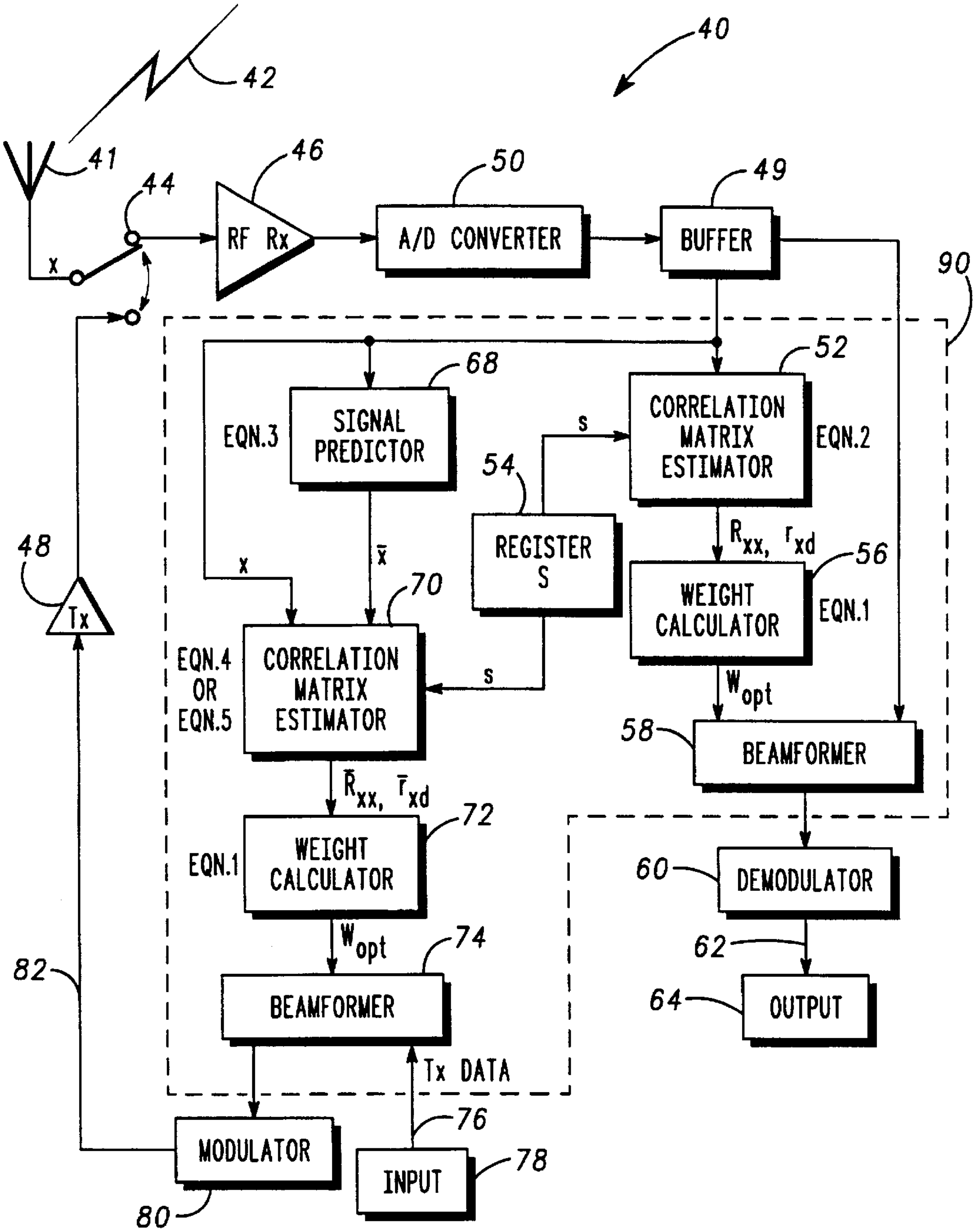

40
42
41
44
x
46
RF Rx
50
A/D CONVERTER
49
BUFFER
90
52
CORRELATION MATRIX ESTIMATOR
EQN.2
68
SIGNAL PREDICTOR
EQN.3
s
54
REGISTER S
R_{xx}, r_{xd}
56
WEIGHT CALCULATOR
EQN.1
48
Tx
x
$\bar{x}$
70
EQN.4 OR EQN.5
CORRELATION MATRIX ESTIMATOR
s
W_{opt}
58
BEAMFORMER
$\bar{R}_{xx}$, $\bar{r}_{xd}$
72
EQN.1
WEIGHT CALCULATOR
60
DEMODULATOR
W_{opt}
74
62
82
BEAMFORMER
64
OUTPUT
Tx DATA
76
MODULATOR
78
INPUT
80

FIG. 3

APPARATUS AND METHOD FOR ADAPTIVE BEAMFORMING IN AN ANTENNA ARRAY

BACKGROUND OF THE INVENTION

This invention relates, in general, to communication systems and is particularly applicable to communication systems using an adaptive beamforming technique.

SUMMARY OF THE PRIOR ART

The use of adaptive antennas (AA) in communication systems (particularly frequency division multiplexed (FDM) systems, such as the pan-European digital cellular Global System for Mobile (GSM) communication and alternate code-division multiple access (CDMA) systems) is becoming increasingly attractive because such adaptive antennas offer general improvements in system performance, and especially handling (traffic) capacity. As will be appreciated, a high degree of beam accuracy is achieved in an adaptive antenna system by accurately varying the phase and amplitude (magnitude) components of a transmitted wave. More specifically, phases and magnitudes of a set of transmitted waves, emanating from an array of antenna elements of a transceiver, are varied by "weighting" individual elements in the array such that an antenna radiation pattern (of a base site, for example) is adapted (optimised) to match prevailing signal and interference environments of a related coverage area, such as a cell.

Adaptive transmit beamforming in duplex communication systems requires that beamforming coefficients (i.e. the "weighting" factors) are adjusted in response to previously received channel information, which received information may occur in either an up-link or down-link for the system. In fact, when specifically considering a GSM base station, beamforming coefficients for a traffic mode must be calculated (estimated) within a period of four time-slot durations (namely a time of $4\times\frac{15}{26}$ milliseconds (ms), nominally 2.3 ms), whereas the period for calculating beamforming coefficients at a mobile unit may, in fact, be of shorter duration. Unfortunately, when one considers the amount of processing required to calculate (estimate) these beamforming coefficients, this limited period of time places severe constraints on an achievable accuracy. Indeed, upon receipt of a signal, information contained within the signal (typically) must be sampled, stored and then demodulated (by synchronisation and equalisation processes). Additionally, transmit weights must be formed from the received signal and then applied to data for transmission prior to loading and modulation of this data.

Furthermore, the limited time available for processing is further eroded by the problems inherently associated with such beamforming mechanisms, which problems principally result from: (i) the beamforming coefficients (weights) being frequency dependent (bearing in mind that the up-link and down-link resources usually operate at different frequencies, such that a frequency transposition and a phase-error correction is required); and (ii) a time dependent fluctuation in channel environment caused by a relative movement between a mobile unit and a fixed base station. In the latter respect, the effects of a time variation may be mitigated to some extent by averaging several received slots weights, for example, but this form of time correction is rather coarse.

With respect to selection of beamforming coefficients in typical communication systems (and as will be understood), an optimum selection (corrected, of course, for differences between the up-link and down-link frequencies) is provided by the Wiener solution:

$$w_{opt}=R_{xx}^{-1}r_{xd} \qquad \text{(eqn. 1)}$$

where:

i) $x=[x_1, x_2, \ldots x_{(n-1)}, x_{(n-2)}]^T$ is a received signal vector at n branches (i.e. n antenna elements);

ii) $w_{opt}=[w_1, w_2, \ldots w_{(n-1)}, w_{(n-2)}]^T$ is a vector of optimum weights for the n branches;

iii) $r_{xd}=E[x^*s]$ is a correlation of a received signal vector with a desired signal vector, s, that is sent during a defined training sequence of a burst;

iv) R_{xx} is the received signal cross-correlation matrix and equals $E[x^*x^T]$;

v) R_{xx}^{-1} represents an inverse matrix for the matrix R_{xx};

vi) x^* is the complex conjugate of x;

vii) T is a vector transposition function in which rows are substituted for columns and vice versa; and

viii) E[.] denotes an expectation value.

The beamforming coefficients necessarily calculated for a succeeding frame of information must be estimated from historic received signals because correlation matrices R_{xx} and r_{xd} are not available directly (inasmuch as one cannot know what these correlation matrices are until such time as a signal relating to these matrices has been received). In this respect, an estimation $\bar{R}_{xx}$. (denoted by the bar) suitable for use in calculating approximate weights for a succeeding frame (n+1) is given by the equation:

$$\bar{R}_{xx}(n+1)=\frac{1}{B}\sum_{k=n-B+1}^{n} x^*(k)x^T(k) \qquad \text{(eqn. 2)}$$

where B is the number of sample portions (such as bursts) that are taken into consideration per estimation (which may, in certain circumstances involve more than one burst per frame), as expressed in the article "Signal Acquisition and Tracking with Adaptive Arrays in the Digital Mobile Radio System IS-54 with Flat-Fading" by J. H. Winters, published in IEEE Transactions on Vehicular Technology in November 1993, 42(4), pages 377–384. As such, an estimation of the correlation matrices is based on actual received signals.

As such, it is desirable, generally, to provide a reliable but improved mechanism (particularly in terms of increased efficiency) by which beamforming coefficients are calculated.

SUMMARY OF THE INVENTION

Apparatus for receiving and transmitting information from an array of adaptive antenna elements, the apparatus comprising storage means for storing received information and characterised by: a predictive filter for estimating, in response to the received information, predicted information likely to be received by the apparatus in at least one future transmission to the apparatus; and means for combining the previously received information and the predicted information to generate beamforming coefficients for weighting information to be transmitted subsequently from the array of adaptive antenna elements, thereby allowing beamforming coefficients to be calculated prior to receipt of information to be received by the apparatus in at least one future transmission to the apparatus.

An a second aspect of the present invention there is provided a method of receiving and transmitting information in an apparatus having an array of adaptive antenna elements, the method comprising the step of storing received information and characterised by the steps of: estimating, in response to the received information, predicted information likely to be received by the apparatus in at least one future transmission to the apparatus; and combining the previously received information and the predicted information to generate beamforming coefficients for weighting information to be transmitted subsequently from the array of adaptive antenna elements, thereby allowing beamforming coefficients to be calculated prior to receipt of information to be received by the apparatus in at least one future transmission to the apparatus.

Exemplary embodiments of the present invention will now be described with reference to the accompanying drawings.

BRIEF DESCRIPTION OF THE DRAWINGS

FIG. **1** is a representation of a prior art duplex communication channel.

FIG. **2** illustrates a relative timing advantage obtained through the implementation of the present invention in relation to processing of the duplex communication channel of FIG. **1**.

FIG. **3** is a functional diagram illustrating a mechanism and apparatus (in accordance with a preferred embodiment of the present invention) for adaptive beamforming.

DETAILED DESCRIPTION OF A PREFERRED EMBODIMENT

Referring to FIG. **1** there is shown a representation of a prior art duplex communication channel **10**, which comprises a plurality of frames **12–18** (in this specific instance only four frames are illustrated for the sake of brevity). Each frame is divided into eight discrete time-slots t_0–t_7 (although it will be appreciated that the number of time-slots may vary according to the system and that each time slot may be of differing duration). As will be understood, the duplex communication channel **10** may be a traffic channel (TCH) or a broadcast control channel (BCCH), with a distinction between these differing forms of channel being realised by the assignment of at least one dedicated time-slot (usually t_0) in the BCCH for system control purposes. If we consider the duplex communication channel **10** to be a TCH, then time-slot t_0 would typically be assigned as a down-link, whereas time-slot t_3 would be assigned to a corresponding up-link. The remaining time-slots would be assigned/paired in a similar fashion. Therefore, in this example, a buffering of two time-slot occurs between down-link transmission and up-link reception in each frame **12–18**, and a buffering **20** of four time-slots (t_4–t_7) occurs between up-link reception and down-link transmission in contiguous frames, as explained above. Clearly, in the case of a mobile unit, the buffering is correspondingly reversed.

According to eqn. 2, a received signal vector, x(k), of a frame k can be derived (from a cross-correlation of bits of a training sequence, such as a known mid-amble sequence in the specific case of GSM) once per burst transmission, while the number of bursts required per estimation, B, is adjusted according to an anticipated rate-of-change of R_{xx}. However, eqn. 2 requires the use of x(n) and is therefore subject to the limited available time between reception and transmission of information by a communication device, e.g. the base station or the mobile unit.

The preferred embodiment of the present invention utilises linear predictive filtering to supply an estimate of received signal samples, $\bar{x}(n)$, likely to be received in the burst immediately preceding a transmission, and combines this estimate with received signal samples obtained from actual (historically received) signals received over an arbitrary (predetermined) number of bursts or frames, e.g. three frames. As will be understood, linear predictive filtering may be modelled on the equation:

$$\bar{x}(n) = \sum_{m=n-M}^{n-1} a_m^T x(m) \qquad \text{(eqn. 3)}$$

where:

i) a_m are the vectors of filter coefficients obtained using techniques known in those of ordinary skill in the art (see the reference book “Adaptive Filter Theory” by Simon Haykin, 2nd Edition, New Jersey, U.S.A.; Prentice-Hall, 1986. ISBN: 0-13-01326-5 for a method of optimising the choice of a_m);

ii) M is a length of the linear predictive filter;

iii) m is an index integer; and

iv) n is the current frame.

Therefore, according to a preferred embodiment of the present invention, an estimation of the correlation matrix is provided by:

$$\bar{R}_{xx}(n+1) = \frac{1}{B}\left(\sum_{k=n-B+1}^{n-1} x^*(k)x^T(k) + \bar{x}^*(n)\bar{x}^T(n)\right) \qquad \text{(eqn. 4)}$$

The mechanism of the present invention therefore allows beamforming coefficients to be calculated in advance of the receipt of a burst (because previously received signals influence subsequent beamforming coefficients), such as before time-slot t_3 in the case of the base station of FIG. **1**. Consequently, additional time-slots are made available for processing between reception and transmission of data, thereby providing increased buffering **30**. This increased buffering is shown in FIG. **2** in which a relative timing advantage obtained through the implementation of the present invention can be seen relative to a corresponding processing time for the duplex communication channel of FIG. **1**. It will be understood that the increased buffering **30** may be an entire frame or greater, but it is at least the additional period provided between the last actual received burst and the burst estimated by the linear predictive filter (which may occur in the same frame).

Although predictive filtering in itself requires processing within a microprocessor (or the like) of a communication device, the additional time provided to the communication device allows either the use of more sophisticated decoding and beamforming algorithms (the latter of which will improve the resolution and accuracy for beamforming within the communication system, generally) or the use of a slower (and hence less expensive) processor. However, the additional processing required in the communication device may be optimised by an appropriate limitation of the number of bursts, B, used during estimation.

For the sake of brevity the mechanism for the calculation of $\bar{R}_{xx}$ has been described in detail, although it will be understood that an identical mathematical approach is preferably adopted for the estimation of $\bar{r}_{xd}$; albeit that appropriate substitutions are required, namely that x^T or $\bar{x}^T$ become s^T.

The basic concept of the present invention may be developed further by weighting each term in eqn. 4 by a factor appropriate to an anticipated rate-of-change of R_{xx}, thereby making the correlation matrix estimation itself predictive.

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